

### Features

- Wide 4.7V to 38V Operating Input Range
- Standoff Voltage: 40V
- 1.0A Continuous Output Current
- 1.1MHz Switching Frequency
- Short Protection with Foldback-Mode
- Built-in Over Current Limit
- Built-in Over Voltage Protection
- Support PSM Mode
- Internal Soft-Start
- 250mΩ/150mΩ Low  $R_{DS(ON)}$  Internal Power MOSFETs
- Output Adjustable from 0.8V
- No Schottky Diode Required
- Integrated internal compensation
- Thermal Shutdown
- Available in SOT23-6 Package
- -40°C to +85°C Temperature Range

### Applications

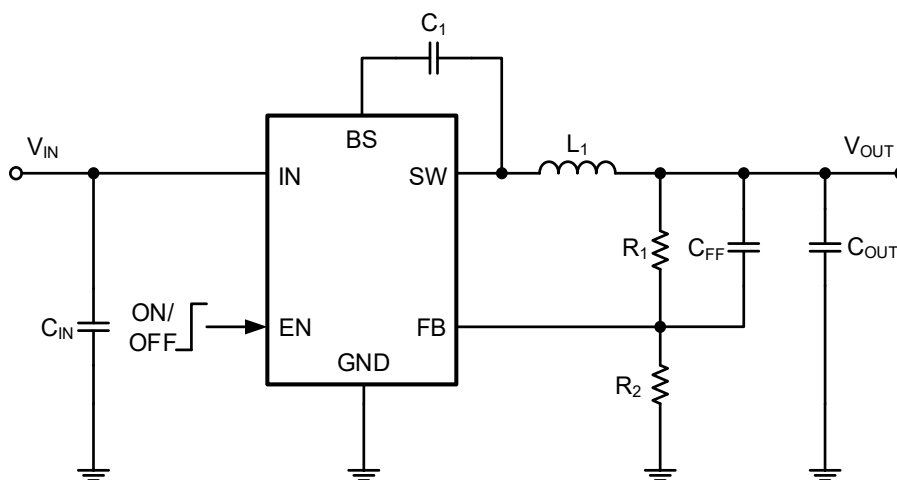
- Battery-Powered Equipment
- Portable Media Players
- Industrial Distributed Power Applications
- Portable Hand-Held Instruments

### General Description

The HE9436 device is high-efficiency, synchronous step-down DC/DC regulators. With a wide input range, it is suitable for a wide range of applications, such as power conditioning from unregulated sources. It features a low  $R_{DS(ON)}$  (250mΩ/150mΩ typical) internal switch for maximum efficiency (92% typical). Supports PSM mode, the operating frequency is fixed at 1.1MHz, allowing the use of small external components while still being able to have low output voltage ripple. With OVP function, the IC can stand off input voltage as high as 40V. The HE9436 supports 1.0A continuous output current, and it has a 0.8V nominal feedback voltage.

Additional features include: thermal shutdown,  $V_{IN}$  undervoltage lockout, and gate drive undervoltage lockout. The HE9436 is available in a low-profile SOT23-6 package.

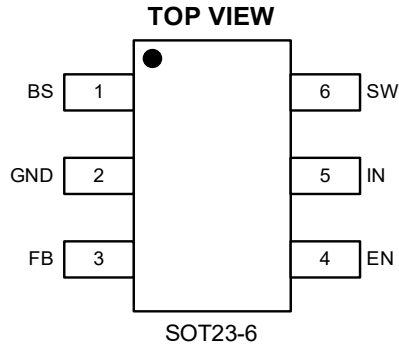
### Typical Application Circuit



Basic Application Circuit

### Pin Description

### Pin Configuration



### Pin Description

Pin	Name	Function
1	BS	Bootstrap. A capacitor connected between SW and BST pins is required to form a floating supply across the high-side switch driver.
2	GND	Ground Pin
3	FB	Adjustable Version Feedback input. Connect FB to the center point of the external resistor divider
4	EN	Drive this pin to a logic-high to enable the IC. Drive to a logic-low to disable the IC and enter micro-power shutdown mode.
5	IN	Power Supply Pin
6	SW	Switching Pin

### Order Information <sup>(1)</sup>

Marking	Part No.	Model	Description	Package	T/R Qty
<u>XXXXX</u>	70301650	HE9436	HE9436 PSM SYN Buck, 4.7-38V, 1.0A, 1.1MHz, VFB 0.8V, SOT23-6	SOT23-6	3000PCS

Note (1): All HEERMICR parts are Pb-Free and adhere to the RoHS directive.

## Specifications

### Absolute Maximum Ratings <sup>(1) (2)</sup>

Item	Min	Max	Unit
V <sub>IN</sub> voltage	-0.3	40	V
EN voltage	-0.3 (V <sub>IN</sub> + 0.3 V)	40	V
SW voltage	-0.3	40	V
BS voltage		7	V
FB voltage	-0.3	6	V
Power dissipation <sup>(3)</sup>	Internally Limited		
Operating junction temperature, T <sub>J</sub>	-40	150	°C
Storage temperature, T <sub>stg</sub>	-65	150	°C
Lead Temperature (Soldering, 10sec.)		260	°C

Note (1): Exceeding these ratings may damage the device.

Note (2): The device is not guaranteed to function outside of its operating conditions.

Note (3): The maximum allowable power dissipation is a function of the maximum junction temperature, T<sub>J(MAX)</sub>, the junction-to-ambient thermal resistance, R<sub>θJA</sub>, and the ambient temperature, T<sub>A</sub>. The maximum allowable power dissipation at any ambient temperature is calculated using: P<sub>D(MAX)</sub> = (T<sub>J(MAX)</sub> - T<sub>A</sub>)/R<sub>θJA</sub>. Exceeding the maximum allowable power dissipation causes excessive die temperature, and the regulator goes into thermal shutdown. Internal thermal shutdown circuitry protects the device from permanent damage. Thermal shutdown engages at T<sub>J</sub>=150°C (typical) and disengages at T<sub>J</sub>= 130°C (typical).

### ESD Ratings

Item	Description	Value	Unit
V <sub>(ESD-HBM)</sub>	Human Body Model (HBM) ANSI/ESDA/JEDEC JS-001-2014 Classification, Class: 2	±2000	V
V <sub>(ESD-CDM)</sub>	Charged Device Mode (CDM) ANSI/ESDA/JEDEC JS-002-2014 Classification, Class: C0b	±200	V
I <sub>LATCH-UP</sub>	JEDEC STANDARD NO.78E APRIL 2016 Temperature Classification, Class: I	±150	mA

### Recommended Operating Conditions

Item	Min	Max	Unit
Operating junction temperature <sup>(1)</sup>	-40	125	°C
Operating temperature range	-40	85	°C
Input voltage V <sub>IN</sub>	4	38	V
Output current	0	1.2	A

Note (1): All limits specified at room temperature (T<sub>A</sub> = 25°C) unless otherwise specified. All room temperature limits are 100% production tested. All limits at temperature extremes are ensured through correlation using standard

Statistical Quality Control (SQC) methods. All limits are used to calculate Average Outgoing Quality Level (AOQL).

### Thermal Information

Item	Description	Value	Unit
R <sub>θJA</sub>	Junction-to-ambient thermal resistance <sup>(1)(2)</sup>	105	°C/W
R <sub>θJC(top)</sub>	Junction-to-case (top) thermal resistance	55	°C/W
R <sub>θJB</sub>	Junction-to-board thermal resistance	17.5	°C/W
ψ <sub>JT</sub>	Junction-to-top characterization parameter	3.5	°C/W
ψ <sub>JB</sub>	Junction-to-board characterization parameter	17.5	°C/W

Note (1): The package thermal impedance is calculated in accordance to JESD 51-7.

Note (2): Thermal Resistances were simulated on a 4-layer, JEDEC board.

### Electrical Characteristics <sup>(1) (2)</sup>

V<sub>IN</sub>=12V, T<sub>A</sub>=25°C, unless otherwise specified.

Parameter	Test Conditions	Min	Typ.	Max	Unit
Input Voltage Range		4.7		38	V
Supply Current (Quiescent)	V <sub>EN</sub> =3.0V		0.4	0.8	mA
Supply Current (Shutdown)	V <sub>EN</sub> =0 or EN = GND			10	uA
Feedback Voltage		0.780	0.800	0.820	V
High-Side Switch On-Resistance	I <sub>SW</sub> =100mA		250		mΩ
Low-Side Switch On-Resistance	I <sub>SW</sub> =-100mA		150		mΩ
Upper Switch Current Limit		2			A
Over Voltage Protection Threshold			39		V
Switching Frequency			1.1		MHz
Maximum Duty Cycle	V <sub>FB</sub> =90%		92		%
Minimum On-Time			90		nS
EN Rising Threshold		1.3			V
EN Falling Threshold				0.9	V
Under-Voltage Lockout Threshold	Wake up V <sub>IN</sub> Voltage		3.6	3.8	V
	Shutdown V <sub>IN</sub> Voltage	3.1	3.3		V
	Hysteresis V <sub>IN</sub> voltage		300		mV
Soft Start			1		mS
Thermal Shutdown			150		°C
Thermal Hysteresis			20		°C

Note (1): MOSFET on-resistance specifications are guaranteed by correlation to wafer level measurements.

Note (2): Thermal shutdown specifications are guaranteed by correlation to the design and characteristics analysis.

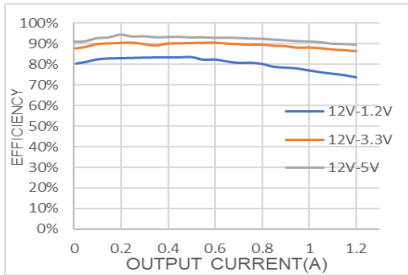
### Typical Performance Characteristics (1) (2)

Note (1): Performance waveforms are tested on the evaluation board.

Note (2):  $V_{IN}=12V$ ,  $V_{OUT}=3.3V$ ,  $T_A = +25^{\circ}C$ , unless otherwise noted.

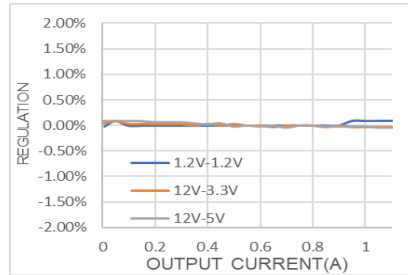
#### Efficiency vs Load Current

$V_{OUT}=5V, 3.3V, 1.2V$



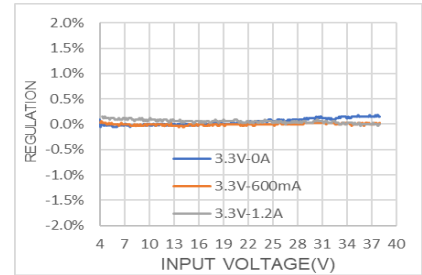
#### Load Regulation

$V_{OUT}=5V, 3.3V, 1.2V$



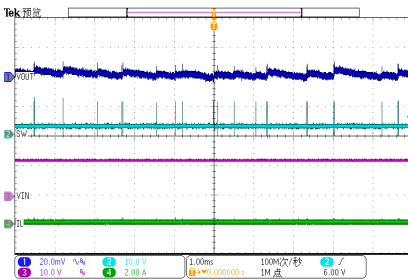
#### Line Regulation

$V_{OUT}=3.3V$



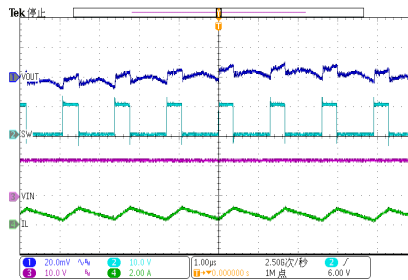
#### Output Ripple Voltage

$V_{IN}=12V, V_{OUT}=3.3V, I_{OUT}=0A$



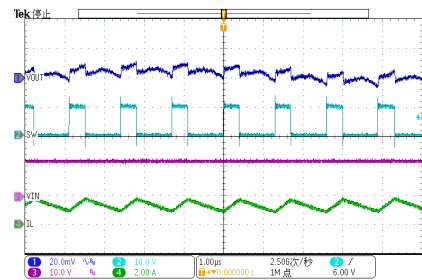
#### Output Ripple Voltage

$V_{IN}=12V, V_{OUT}=3.3V, I_{OUT}=0.6A$



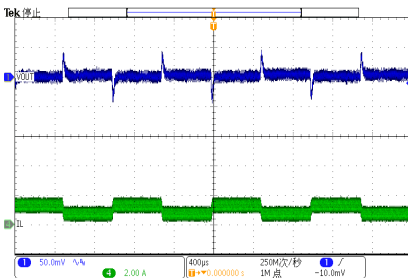
#### Output Ripple Voltage

$V_{IN}=12V, V_{OUT}=3.3V, I_{OUT}=1.0A$



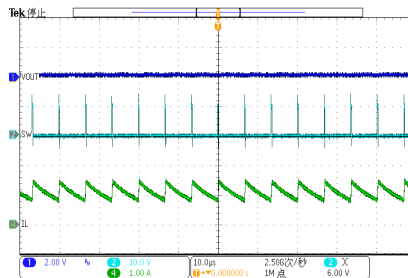
#### Loop Response

$V_{IN}=12V, V_{OUT}=3.3V, I_{OUT}=0.6A-1.0A$



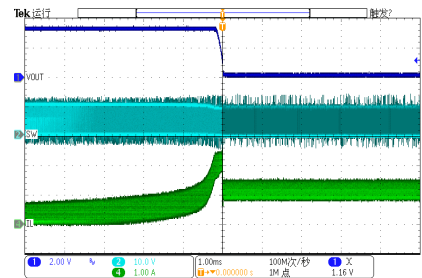
#### Output Short

$V_{IN}=12V, V_{OUT}=3.3V$



#### Short Circuit Entry

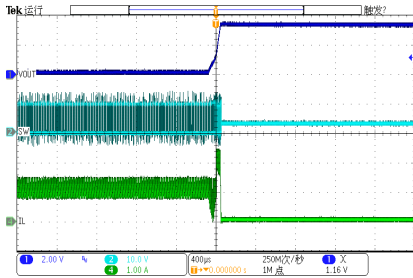
$V_{IN}=12V, V_{OUT}=3.3V$



**40V, 1.0A synchronous Step-Down Converter**

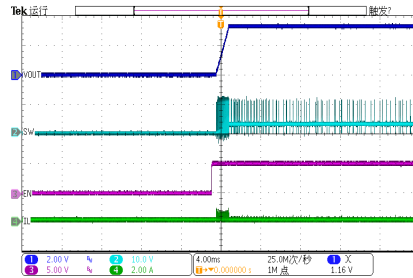
**Short Circuit Recovery**

$V_{IN}=12V, V_{OUT}=3.3V$



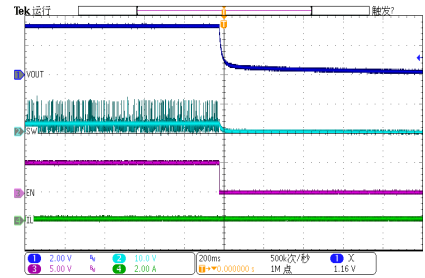
**Enable Startup at No Load**

$V_{IN}=12V, V_{OUT}=3.3V, I_{OUT}=0A$



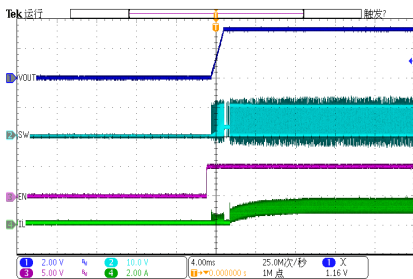
**Enable Shutdown at No Load**

$V_{IN}=12V, V_{OUT}=3.3V, I_{OUT}=0A$



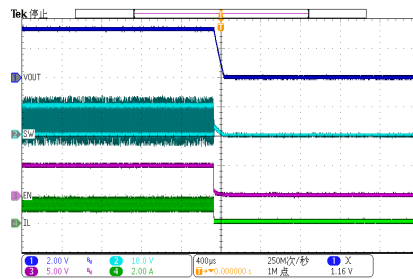
**Enable Startup at Full Load**

$V_{IN}=12V, V_{OUT}=3.3V, I_{OUT}=1.0A$



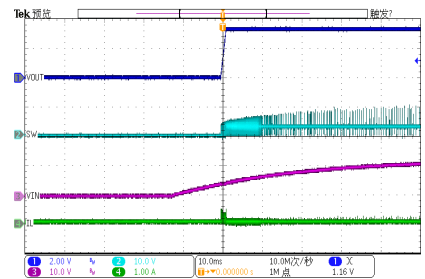
**Enable Shutdown at Full Load**

$V_{IN}=12V, V_{OUT}=3.3V, I_{OUT}=1.0A$



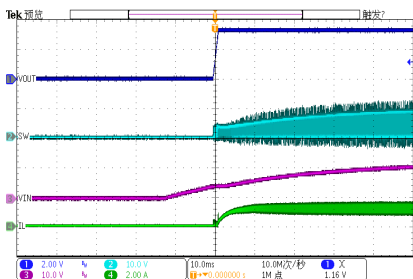
**Power Up at No Load**

$V_{IN}=12V, V_{OUT}=3.3V, I_{OUT}=0A$

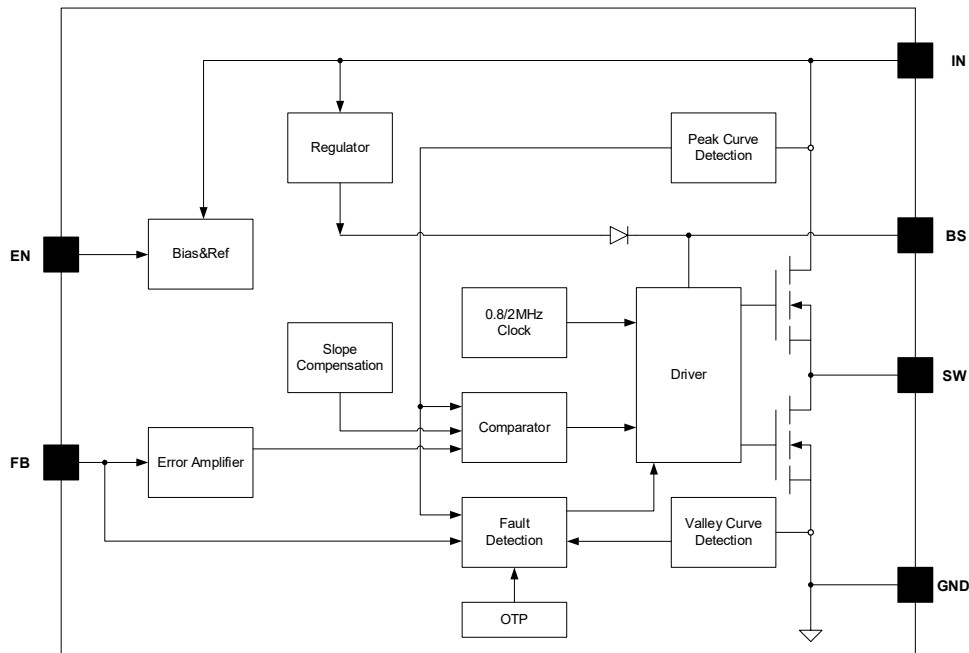


**Power Up at Full Load**

$V_{IN}=12V, V_{OUT}=3.3V, I_{OUT}=1.0A$



## Functional Block Diagram



Block Diagram

## Functions Description

### Internal Regulator

The HE9436 is a current mode step down DC/DC converter that provides excellent transient response with no extra external compensation components. This device contains an internal, low resistance, high voltage power MOSFET, and operates at a high 1.1MHz operating frequency to ensure a compact, high efficiency design with excellent AC and DC performance.

### Error Amplifier

The error amplifier compares the FB pin voltage with the internal FB reference ( $V_{FB}$ ) and outputs a current proportional to the difference between the two. This output current is then used to charge or discharge the internal compensation network, which is used to control the power MOSFET current. The optimized internal compensation network minimizes the external component counts and simplifies the control loop design.

### Under-Voltage Lockout (UVLO)

Under-voltage lockout (UVLO) protects the chip from operating at an insufficient supply voltage. UVLO protection monitors the internal regulator voltage. When the voltage is lower than UVLO threshold voltage, the device is shut off. When the voltage is higher than UVLO threshold voltage, the device is enabled again.

### Thermal Shutdown

Thermal shutdown prevents the chip from operating at exceedingly high temperatures. When the silicon die temperature exceeds 150°C, it shuts down the whole chip. When the temperature falls below its lower threshold (Typ. 130°C) the chip is enabled again.

**Internal Soft-Start**

The soft-start is implemented to prevent the converter output voltage from overshooting during startup. When the chip starts, the internal circuitry generates a soft-start voltage (SS) ramping up from 0V to 0.8V. When it is lower than the internal reference (REF), SS overrides REF so the error amplifier uses SS as the reference. When SS is higher than REF, REF regains control. The SS time is internally max to 1ms.

**Over Current Protection with Foldback**

The HE9436 has cycle-by-cycle over current limit when the inductor current peak value exceeds the set current limit threshold. Meanwhile, output voltage starts to drop until FB is below the Under-Voltage (UV) threshold. When the output is shorted to the ground, the switching frequency is folded back and the current limit is reduced to lower the short circuit current. The frequency foldback helps prevent inductor current runaway and thermal issue during short circuit. The HE9436 exits the foldback mode once the over current condition is removed.

**Startup and Shutdown**

If both  $V_{IN}$  and EN are higher than their appropriate thresholds, the chip starts. The reference block starts first, generating stable reference voltage and currents, and then the internal regulator is enabled. The regulator provides stable supply for the remaining circuitries. Three events can shut down the chip: EN low,  $V_{IN}$  low and thermal shutdown. In the shutdown procedure, the signaling path is first blocked to avoid any fault triggering. The comp voltage and the internal supply rail are then pulled down. The floating driver is not subject to this shutdown command.



## Applications Information

### Setting the Output Voltage

HE9436 require an input capacitor, an output capacitor and an inductor. These components are critical to the performance of the device. HE9436 integrates internal loop compensating resistors, so we do not recommend using a value of more than 50K for R<sub>2</sub>. The output voltage can be programmed by resistor divider.

$$V_{OUT} = V_{FB} \times \frac{R1 + R2}{R2}$$

V <sub>OUT</sub> (V)	R1(KΩ)	R2(KΩ)	L1(μH)	C1(nF)	C <sub>IN</sub> (μF)	C <sub>OUT</sub> (μF)	C <sub>FF</sub> (pF) Opt.
1.0	12.5	50	2.2	100	22	22×2	<a href="#">C<sub>FF</sub> Chapter</a>
1.05	15.65	50	2.2	100	22	22×2	<a href="#">C<sub>FF</sub> Chapter</a>
1.2	25.0	50	2.2	100	22	22×2	<a href="#">C<sub>FF</sub> Chapter</a>
1.5	43.75	50	2.2	100	22	22×2	<a href="#">C<sub>FF</sub> Chapter</a>
1.8	62.5	50	3.3	100	22	22×2	<a href="#">C<sub>FF</sub> Chapter</a>
2.5	106.25	50	3.3	100	22	22×2	<a href="#">C<sub>FF</sub> Chapter</a>
3.3	156.25	50	4.7	100	22	22×2	<a href="#">C<sub>FF</sub> Chapter</a>
5.0	262.5	50	4.7	100	22	22×2	<a href="#">C<sub>FF</sub> Chapter</a>

All the external components are the suggested values, the final values are based on the application testing results.

### Selecting the Inductor

The recommended inductor values are shown in the Application Diagram. It is important to guarantee the inductor core does not saturate during any foreseeable operational situation. The inductor should be rated to handle the maximum inductor peak current: Care should be taken when reviewing the different saturation current ratings that are specified by different manufacturers. Saturation current ratings are typically specified at 25°C, so ratings at maximum ambient temperature of the application should be requested from the manufacturer. The inductor value can be calculated with:

$$L = \frac{V_{OUT} \times (V_{IN} - V_{OUT})}{V_{IN} \times \Delta I_L \times F_{OSC}}$$

Where ΔI<sub>L</sub> is the inductor ripple current. Choose inductor ripple current to be approximately 30% to 40% of the maximum load current. The maximum inductor peak current can be estimated as:

$$I_{L(MAX)} = I_{LOAD} + \frac{\Delta I_L}{2}$$

Under light load conditions below 100mA, larger inductance is recommended for improved efficiency. Larger inductances lead to smaller ripple currents and voltages, but they also have larger physical dimensions, lower saturation currents and higher linear impedance. Therefore, the choice of inductance should be compromised according to the specific application.

### Selecting the Input Capacitor

The input current to the step-down converter is discontinuous and therefore requires a capacitor to supply AC current to the step-down converter while maintaining the DC input voltage. For a better performance, use ceramic capacitors placed as close to VIN as possible and a 0.1μF input capacitor to filter out high frequency interference is recommended. Capacitors with X5R and X7R ceramic dielectrics are recommended because they are stable with temperature fluctuations.

The capacitors must also have a ripple current rating greater than the maximum input ripple current of the converter. The input ripple current can be estimated with Equation:

$$I_{CIN} = I_{OUT} \times \sqrt{\frac{V_{OUT}}{V_{IN}} \times \left(1 - \frac{V_{OUT}}{V_{IN}}\right)}$$

From the above equation, it can be concluded that the input ripple current reaches its maximum at  $V_{IN}=2V_{OUT}$  where  $I_{CIN} = \frac{I_{OUT}}{2}$ . For simplification, choose an input capacitor with an RMS current rating greater than half of the maximum load current.

The input capacitance value determines the input voltage ripple of the converter. If there is an input voltage ripple requirement in the system, choose the input capacitor that meets the specification. The input voltage ripple can be estimate with Equation:

$$\Delta V_{IN} = \frac{I_{OUT}}{F_{OSC} \times C_{IN}} \times \frac{V_{OUT}}{V_{IN}} \times \left(1 - \frac{V_{OUT}}{V_{IN}}\right)$$

Similarly, when  $V_{IN}=2V_{OUT}$ , input voltage ripple reaches its maximum of  $\Delta V_{IN} = \frac{1}{4} \times \frac{I_{OUT}}{F_{OSC} \times C_{IN}}$ .

### Selecting the Output Capacitor

An output capacitor is required to maintain the DC output voltage. The output voltage ripple can be estimated with Equation:

$$\Delta V_{OUT} = \frac{V_{OUT}}{F_{OSC} \times L} \times \left(1 - \frac{V_{OUT}}{V_{IN}}\right) \times \left(R_{ESR} + \frac{1}{8 \times F_{OSC} \times C_{OUT}}\right)$$

There are some differences between different types of capacitors. In the case of ceramic capacitors, the impedance at the switching frequency is dominated by the capacitance. The output voltage ripple is mainly caused by the capacitance. For simplification, the output voltage ripple can be estimated with Equation:

$$\Delta V_{OUT} = \frac{V_{OUT}}{8 \times F_{OSC}^2 \times L \times C_{OUT}} \times \left(1 - \frac{V_{OUT}}{V_{IN}}\right)$$

A larger output capacitor can achieve a better load transient response, but the maximum output capacitor limitation should also be considered in the design application. If the output capacitor value is too high, the output voltage will not be able to reach the design value during the soft-start time and will fail to regulate. The maximum output capacitor value ( $C_{OUT\_MAX}$ ) can be limited approximately with Equation:

$$C_{OUT\_MAX} = (I_{LIM\_AVG} - I_{OUT}) \times T_{SS}/V_{OUT}$$

Where  $L_{LIM\_AVG}$  is the average start-up current during the soft-start period, and  $T_{SS}$  is the soft- start time.

On the other hand, special attention should be paid when selecting these components. The DC bias of these capacitors can result in a capacitance value that falls below the minimum value given in the recommended capacitor specifications table.

The ceramic capacitor's actual capacitance can vary with temperature. The capacitor type X7R, which operates over a temperature range of  $-55^{\circ}\text{C}$  to  $+125^{\circ}\text{C}$ , will only vary the capacitance to within  $\pm 15\%$ . The capacitor type X5R has a similar tolerance over a reduced temperature range of  $-55^{\circ}\text{C}$  to  $+85^{\circ}\text{C}$ . Many large value ceramic capacitors, larger than  $1\mu\text{F}$  are manufactured with Z5U or Y5V temperature characteristics. Their capacitance can drop by more than 50% as the temperature varies from  $25^{\circ}\text{C}$  to  $85^{\circ}\text{C}$ . Therefore, X5R or X7R is recommended over Z5U and Y5V in applications where the ambient temperature will change significantly above or below  $25^{\circ}\text{C}$ .

### **Feed-Forward Capacitor ( $C_{FF}$ )**

HE9436 has internal loop compensation, so adding  $C_{FF}$  is optional. Specifically, for specific applications, if necessary, consider whether to add feed-forward capacitors according to the situation.

The use of a feed-forward capacitor ( $C_{FF}$ ) in the feedback network is to improve the transient response or higher phase margin. For optimizing the feed-forward capacitor, knowing the cross frequency is the first thing. The cross frequency (or the converter bandwidth) can be determined by using a network analyzer. When getting the cross frequency with no feed-forward capacitor identified, the value of feed-forward capacitor ( $C_{FF}$ ) can be calculated with the following Equation:

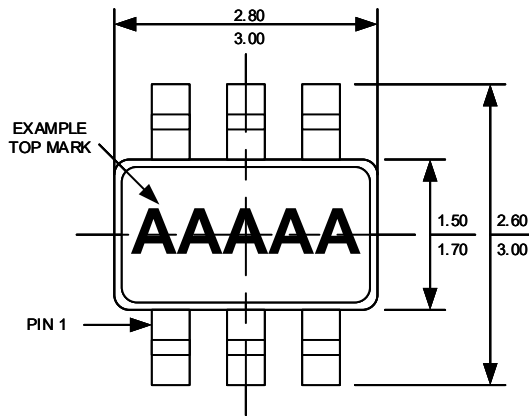
$$C_{FF} = \frac{1}{2\pi \times F_{CROSS}} \times \sqrt{\frac{1}{R1} \times \left(\frac{1}{R1} + \frac{1}{R2}\right)}$$

Where  $F_{CROSS}$  is the cross frequency.

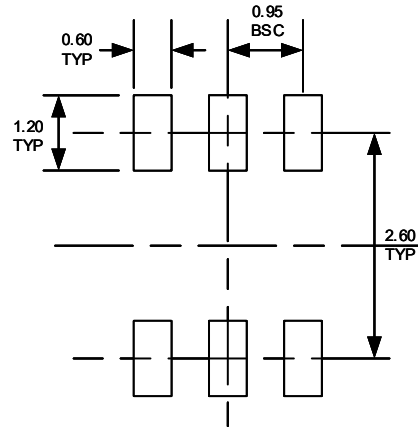
To reduce transient ripple, the feed-forward capacitor value can be increased to push the cross frequency to higher region. Although this can improve transient response, it also decreases phase margin and cause more ringing. In the other hand, if more phase margin is desired, the feed-forward capacitor value can be decreased to push the cross frequency to lower region.

**Package Description**

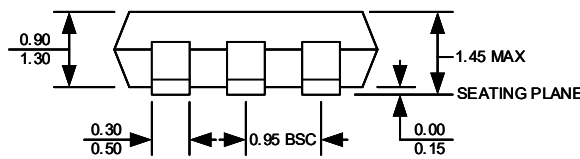
**SOT23-6**



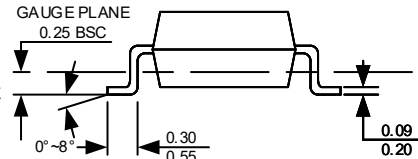
**TOP VIEW**



**RECOMMENDED PAD LAYOUT**



**FRONT VIEW**



**SIDE VIEW**